Evaluation of niobium transmission lines up to the superconducting gap frequency


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The frequency dependence of the coupling of niobium superconducting transmission lines is measured for frequencies up to and above the superconducting gap frequency. For this purpose superconducting microstrips are integrated in log-periodic planar antennas and the spectral response is measured by means of a Fourier transform spectrometer with 1 μm² Nb/Al₂O₃/Nb SIS junctions as detectors. Resonances of microstrips are observed up to 650 GHz, the superconducting gap frequency of niobium, but above that frequency no resonances have been detected. The measured resonance frequencies are in good agreement with a dispersive model for superconducting transmission lines based on the Mattis–Bardeen theory. The radiation coupling is lower than calculated, indicating significant dielectric losses.

Superconducting transmission lines (stubs) are often used as an integrated tuning and matching network for superconducting tunnel junctions in mixers and detectors. In a waveguide mixer the geometrical capacitance of the junction can be additionally tuned by a backshort and an E-plane tuner. On a planar antenna, however, this capacitance can only be compensated by means of an integrated tuning network. The integrated tuning elements exist usually out of superconducting striplines. Until recently, dimensions of the structure are scaled down in size for higher frequencies, while very few results are published about the behavior of niobium above or close to the gap frequency.¹-³ Loss at this frequency can limit the use of transmission lines made out of niobium. In this paper we will compare calculated with measured resonances from a stub parallel to a junction and identify some problems which will arise at these high frequencies.

The first published measurements of integrated tuning elements used the self-pumped steps in I-V characteristics to measure the resonance of a stub.⁴ A more accurate and complete evaluation can be achieved with a Michelson interferometer used as a Fourier transform spectrometer (FTS).⁵ The source is a broad-band mercury arc lamp. In our case the usable frequency range is limited by a 50 μm thick kapton beam splitter and ranges from 150 to 1000 GHz. The spectral response of our device is derived from the current variation of the junction as a function of path-length difference of the Michelson. The Fourier transform of this interferogram yields the frequency response of the detector.

We use two junctions in series of each 1 μm² area and a critical current density of 12000 A/cm² and we assume a specific capacitance of 55 pF/μm². The junctions are fabricated with the selective niobium over-etch process. (SNOEP).⁶ The wiring layer on top of the junctions includes a stub for each junction. Both the antenna and the stub are made of niobium and are assumed to have a penetration depth of 100 nm.⁷ The dielectric layer between the ground plane (antenna) and the stub is 250 nm thick sputtered SiO₂. The devices are fabricated on a 200 μm thick fused quartz substrate.

A stub length of 500 μm and a width of 5 μm results in our case in a fundamental resonance around 100 GHz and harmonic resonances at multiple frequencies. The antenna is glued to a quartz lens and mounted in a liquid helium bath Dewar with only dc bias connections.

For an interpretation of the measured spectra we assume that the junction can be described at rf frequencies by the quantum impedance parallel to its geometrical capacitance. The quantum impedance is calculated using the equations from Tucker and Feldman⁸ assuming the experiment is working in the small signal limit. This means that we can neglect dependency on incident power. The characteristic impedance of the stub is calculated using the well-known equations for superconducting transmission lines.⁹ We include the loss (α) and dispersion (β) of niobium as a function of frequency in the calculation. Both parameters are calculated according to the paper of Kautz.¹⁰ This is based on the theory of Mattis and Bardeen.¹¹ The impedance of the stub follows from¹²

\[ Z = \frac{Z₀}{\tanh(γl)} \]  

where \( Z₀ \) is the characteristic impedance of the transmission line, \( l \) is the length, and \( γ = α + iβ \) is the propagation constant. In Eq. (1) we take into account the frequency dependency of \( Z₀ \) and \( γ \). The coupling coefficient \( C₀ \) is defined as the fraction of the available power dissipated in the junction:

\[ C₀ = \frac{Z₀ - Z}{Z₀} \]
where the impedance of the antenna is approximated by $Z_{ant} = 120 \, \Omega$, $Y_{ant} = 1/Z_{ant}$, $Y_j$ is the admittance of the junction with the stub in parallel, and $\ast$ denotes the complex conjugate.

The electric equivalent of the structure is shown in Fig. 1. The radiation source is approximated by a current source $I_S$ parallel to the antenna impedance. The leads inductance $L_{leads}$ between the junctions can be neglected in the calculation. Each junction is represented by its geometrical capacitance $C_j$ parallel to its quantum impedance ($G_Q + fB_Q$). The stub impedance is represented by $B_S$.

Because of the frequency dependency of the photon energy, the responsivity of the junction as a function of its $I$-$V$ characteristic and frequency should also be taken into account. The junction responsivity $R$ is determined by:

$$ R = \frac{e}{\hbar \omega} \frac{I_{dc}(V_0 + \hbar \omega/e) - 2I_{dc}(V_0) + I_{dc}(V_0 - \hbar \omega/e)}{I_{dc}(V_0 + \hbar \omega/e) - I_{dc}(V_0 - \hbar \omega/e)}, $$

where $\omega$ is the frequency, $e$ is the electron charge, and $I_{dc}$ is the dc current of the junction at the bias voltage $V_0$.

Using Eqs. (2) and (3), the response of the detector to the incident radiation as a function of frequency and bias voltage can be calculated.

Figure 2 shows the coupling $C_{st}$ calculated for a device with a lossless stripline (dotted line) compared to a structure with a lossy stub according to Mattis-Bardeen theory (dashed line) as a function of frequency. These results are compared with a measurement of a structure with a 500 $\mu$m long niobium stub. For reference the gap frequency of niobium (650 GHz) is indicated by a dash-dotted line.

A comparison between the calculations and the measurements for niobium shows a fairly good agreement above 200 GHz. Apparently the dispersion is very well predicted by the theory but the coupling shows more loss than we calculated. This may be caused by losses in the dielectric, because the absorption of fused quartz is fairly high for frequencies of about 1 up to around 100 THz. Obviously, sputtered quartz has more losses and this can explain the extra loss in coupling. The extra loss cannot be explained by the antenna coupling, because it has a flat response from 150 to around 800 GHz.

For improved coupling above the gap frequency both the niobium electrodes as well as the $SiO_2$ dielectric should be replaced by different materials. Niobium can be replaced by NbN or by a normal metal, e.g., gold, because they have less loss at these frequencies. For the dielectric, separate measurements should be performed for carefully determining its properties.

In conclusion, the resonances of niobium stubs with Nb/$Al_2O_3$/Nb junctions are measured and modeled. We can explain the observed frequency dependency of the coupling by taking into account the junction quantum impedance, its responsivity, and the loss and dispersion of niobium as known from the Mattis-Bardeen theory. We do observe more loss than calculated, which may be caused by dielectric losses in the sputtered $SiO_2$ layer. In the measurements we do not observe clear resonances above the gap frequency of niobium (650 GHz). This is in agreement with our model calculations.

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